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**Crawford**

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(54) **TRANSMISSION SECURITY FOR WIRELESS COMMUNICATIONS**

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(52) **U.S. Cl.** ..... **455/410**; 370/203; 380/274

(58) **Field of Search** ..... 370/203, 205, 370/210; 380/270-274; 455/410, 411

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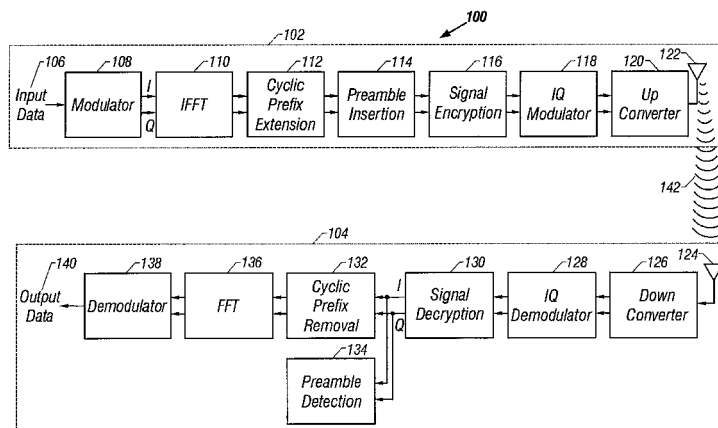
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(57) **ABSTRACT**

A method of transmission level security, and a corresponding transmission security system, the method consists of the steps of: forming a plurality of digital signals representing a symbol to be transmitted over a communication medium, wherein respective ones of the plurality of digital signals are modulated onto respective ones of a plurality of subcarriers according to a multiple carrier modulation scheme; and introducing a group delay distortion in one or more of the plurality of subcarriers, wherein a peak-to-peak variation of the group delay distortion is greater than a guard time interval corresponding to the symbol, such that portions of the one or more of the plurality of subcarriers will be received outside of a time window corresponding to the symbol at a receiver.

**32 Claims, 7 Drawing Sheets**



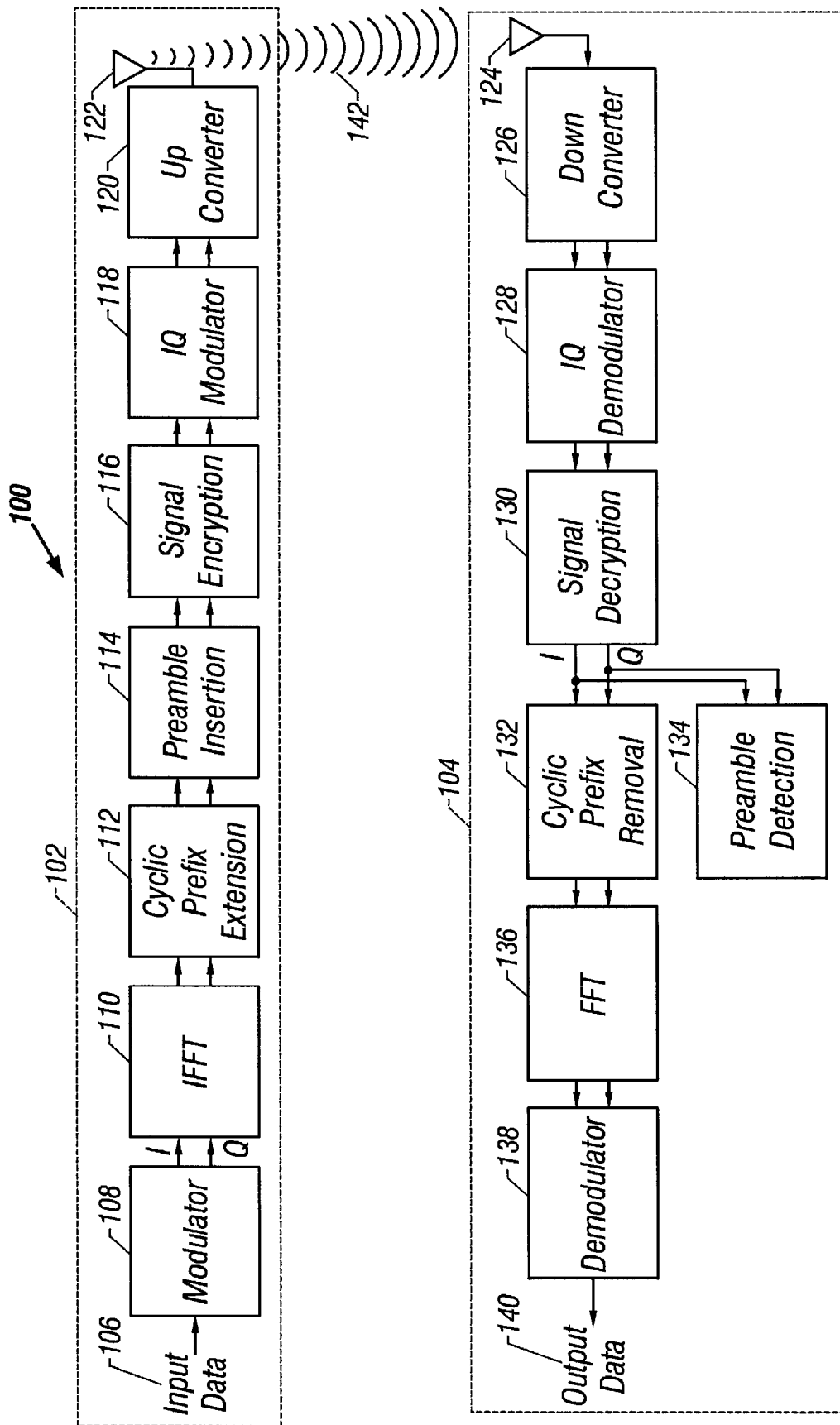


FIG. 1

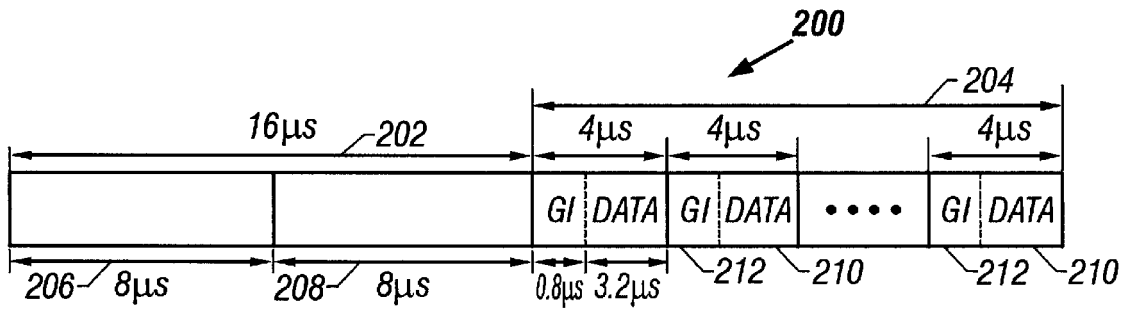
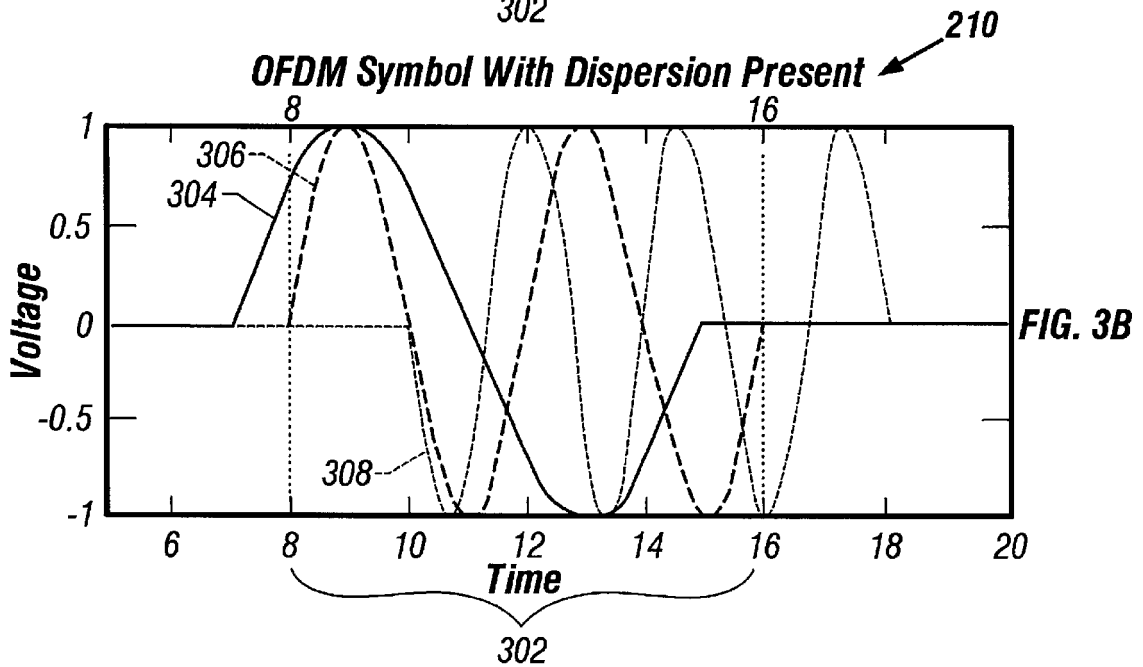
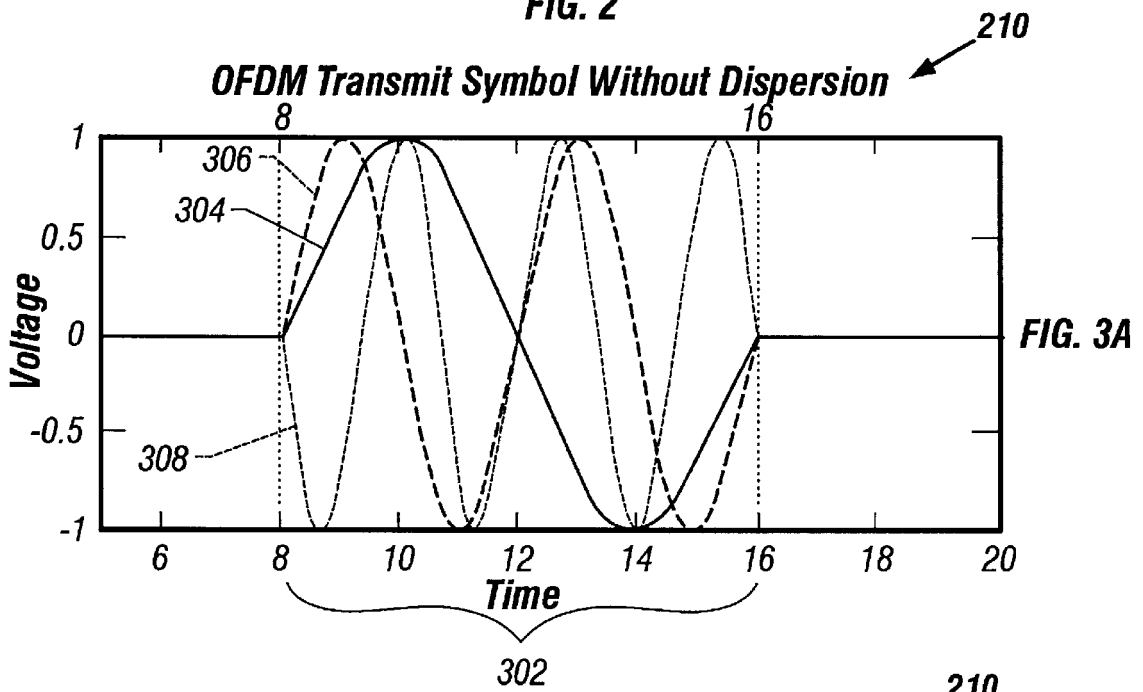


FIG. 2



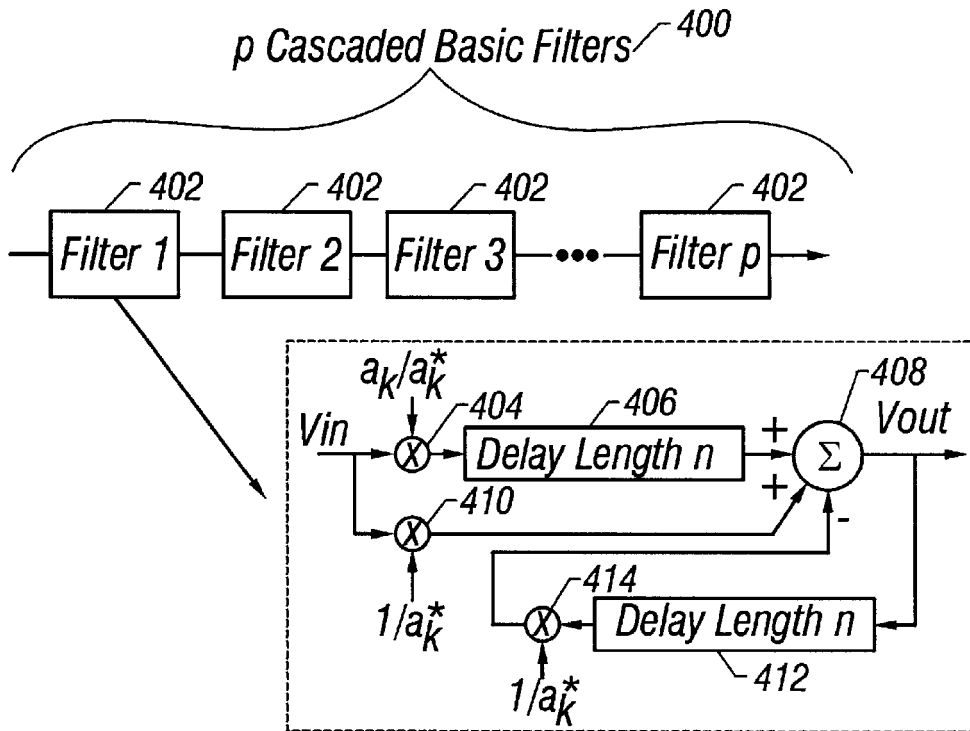


FIG. 4

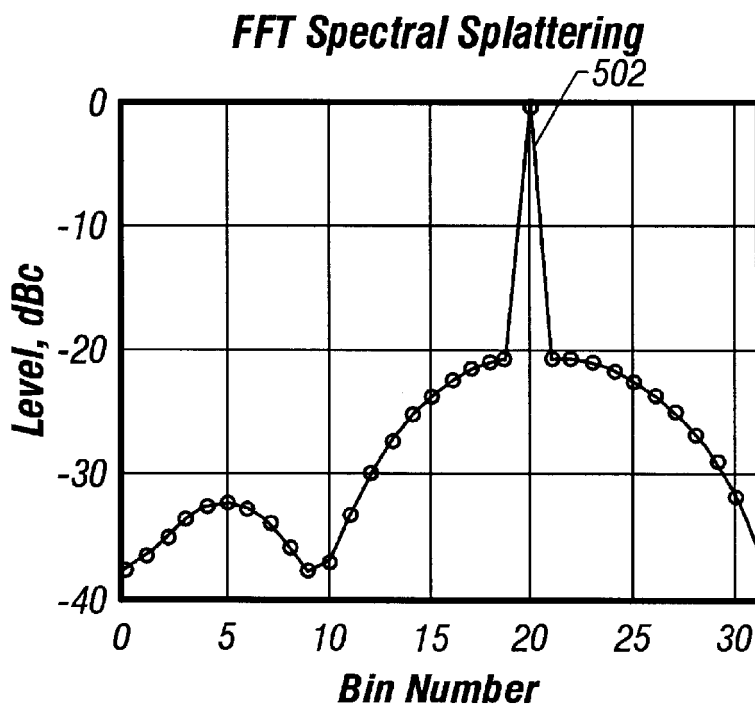
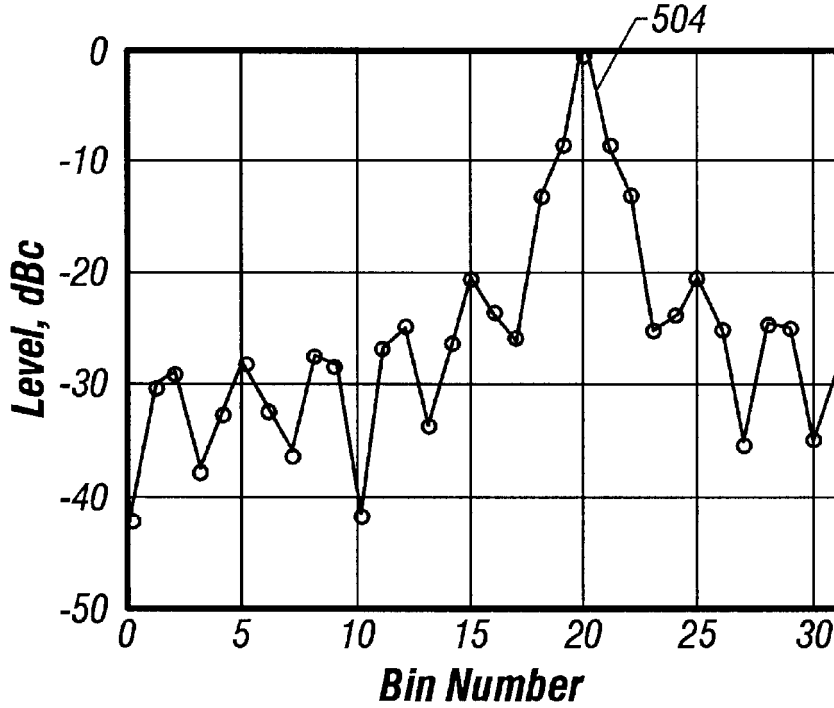


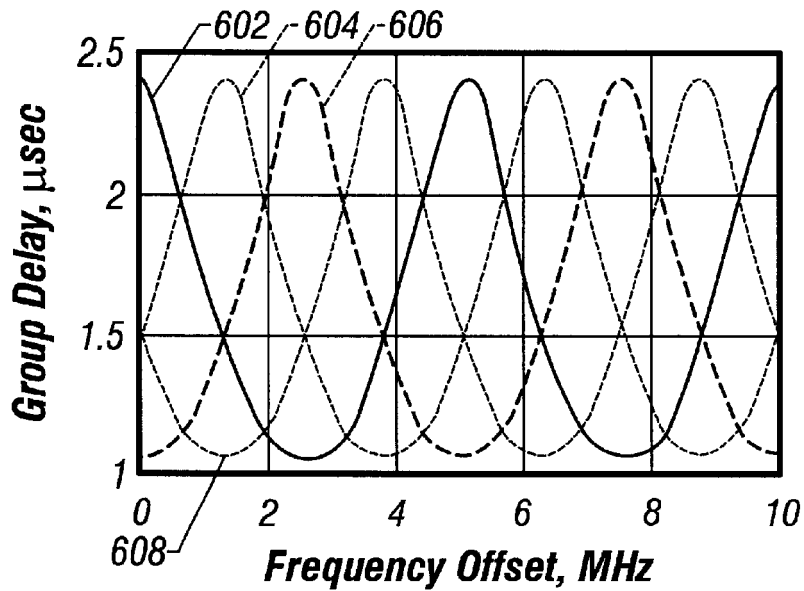
FIG. 5A

**FFT Spectral Splattering**

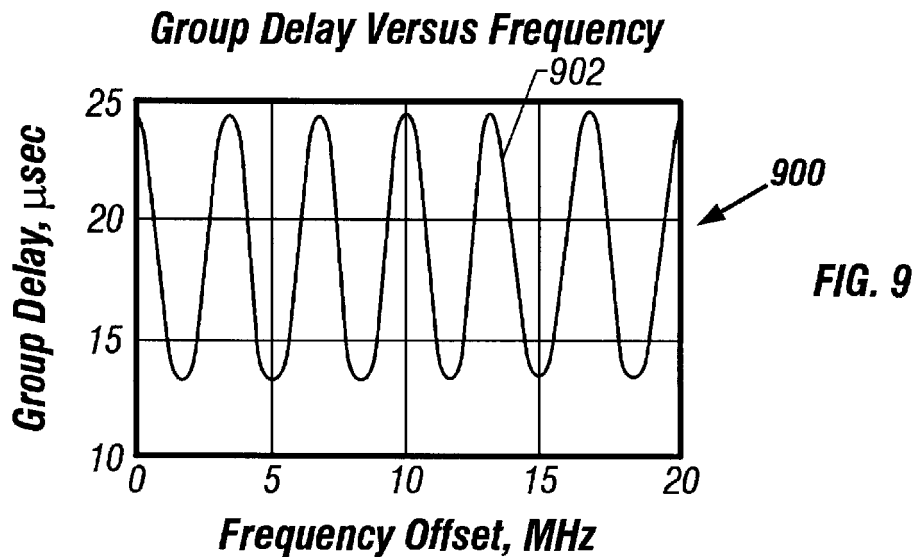
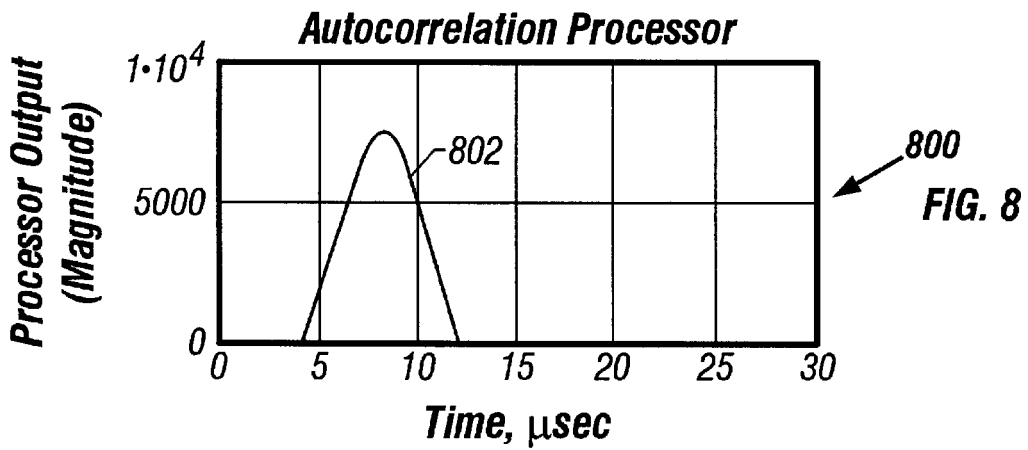
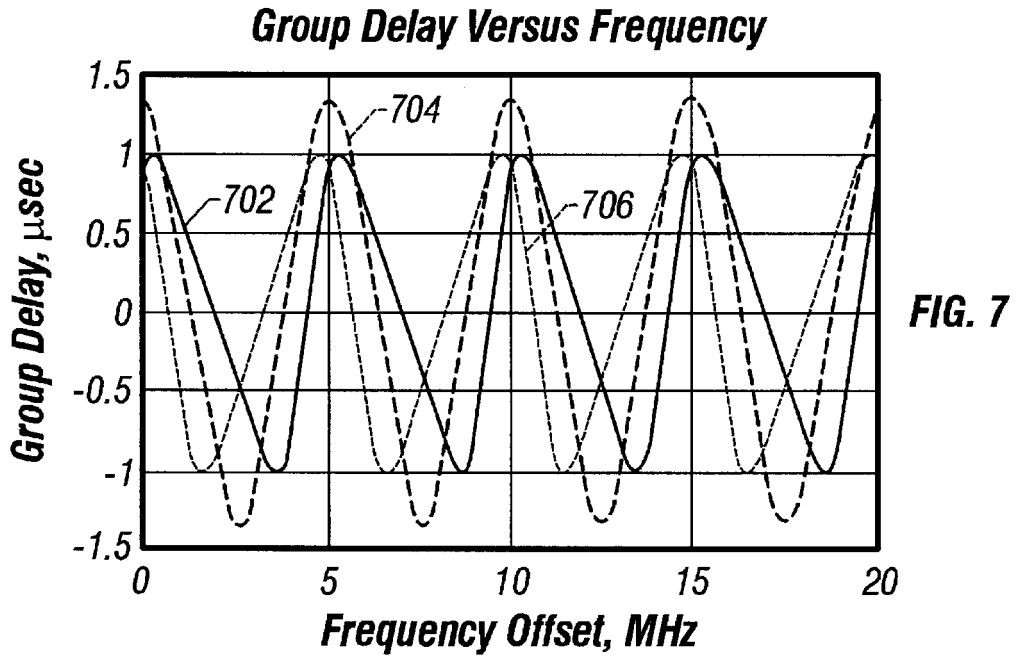


**FIG. 5B**

**Group Delay Versus Frequency**



**FIG. 6**



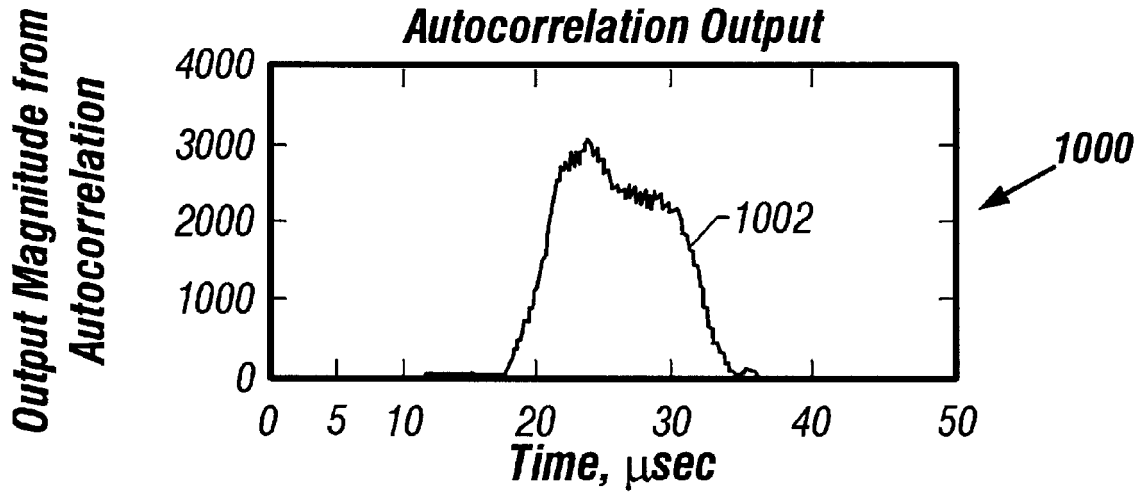


FIG. 10

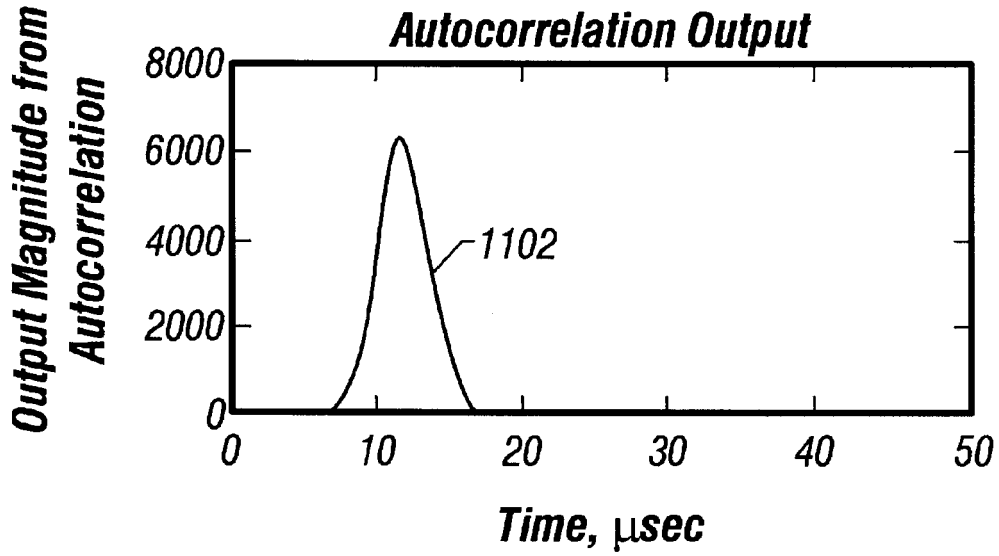


FIG. 11

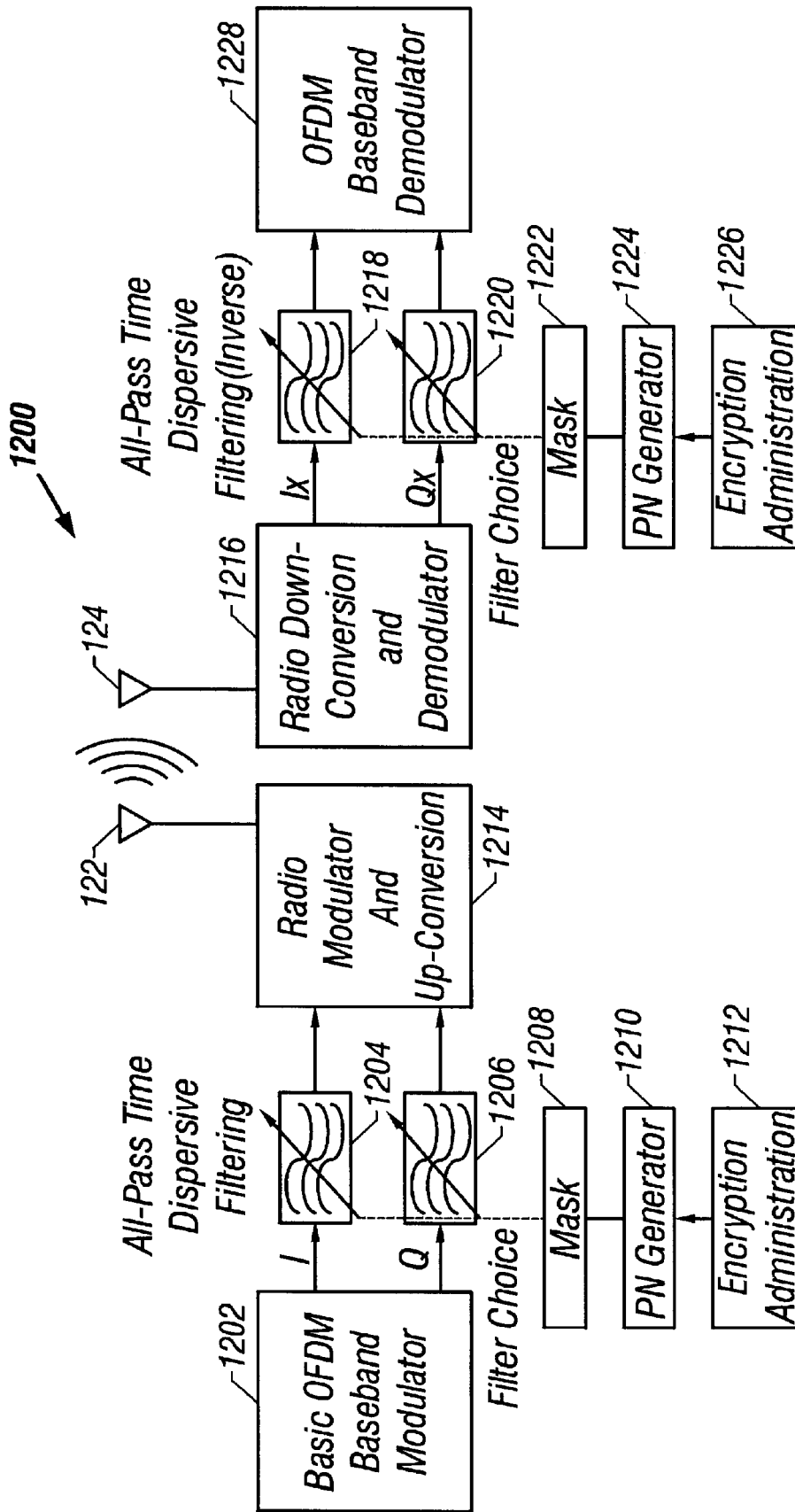


FIG. 12



## TRANSMISSION SECURITY FOR WIRELESS COMMUNICATIONS

### BACKGROUND OF THE INVENTION

#### 1. Field of the Invention

The present invention relates to security for communication systems and more specifically to transmission level security for communication systems using multiple carrier modulation techniques. Even more specifically, the present invention relates to transmission level security for communication systems using multiple carrier modulation techniques, such as orthogonal frequency division multiplexing (OFDM).

2. Discussion of the Related Art security is becoming increasingly important in communications systems which transmit data. Wireline communication systems, such as coaxial cable and especially fiber optic cable, are inherently secure since such mediums must be physically tapped to intercept data transmissions. On the other hand, wireless data transmission is inherently insecure, since data is transmitted openly over an air interface such that an unauthorized entity may easily intercept the transmission. In the context of wireless local area network (LAN) applications, security is extremely important since sensitive data is transmitted to and from multiple devices that constitute the network. Without any security measures, eavesdroppers may freely receive data transmissions between devices in the wireless LAN. As such, transmission security is required to ensure that unauthorized entities are not allowed to intercept the data as it is communicated across the network.

Many bit-level security technologies exist in which the data is encrypted prior to transmission over the wireless medium. Typically, encryption involves scrambling the data bits prior to transmission and the receivers in the network are provided with the logic to decrypt the transmitted information. Common bit-level security techniques include DPF (Data Private Facility) and DES (Data Encryption Standard). These encryption techniques make use of either a Public Key or a Private Key which is used by authorized receivers to decrypt the data. As such, without the key, unauthorized users have a difficult time descrambling the data.

Many bit-level security measures, for example, those used in OFDM (Orthogonal Frequency Division Multiplexed) wireless LAN applications using the HiperLAN2 and IEEE802.11 standards, offer data payload level encryption to encrypt the data but transmit the preambles and control fields with no protection. Thus, an unauthorized eavesdropper can easily intercept the data, although it is encrypted. Disadvantageously, having received the data, the unauthorized eavesdropper can easily parse the data fields from the PHY-layer communications and possibly reverse engineer the encryption technique and extract the underlying source information.

Another form of security is transmission-level security in which the physical waveform (i.e. PHY-layer) carrying the data is altered according to an encryption technique. Advantageously, since the physical waveform is altered, unauthorized eavesdroppers may not even be able to meaningfully receive the transmitted signal at all. One conventional transmission-level encryption technique includes frequency hopping in which the carrier frequency that carries the data is periodically hopped between several different frequencies in a pseudo random fashion. Unless an eavesdropper is aware of the frequencies used and the hopping pattern, the eavesdropper will be unable to receive the transmitted data.

### SUMMARY OF THE INVENTION

The present invention advantageously addresses the needs above as well as other needs by providing a transmission level security technique which introduces a known group delay distortion into the transmitted signaling, which for the unequipped receiver, will interfere with the reception of data and in some embodiments, interfere with the detection and acquisition of the preamble for the frame carrying the data.

In one embodiment, the invention can be characterized as a method of transmission level security in a communication system, and a means for accomplishing the method, the method including the steps of: forming a plurality of digital signals representing a symbol to be transmitted over a communication medium, wherein respective ones of the plurality of digital signals are modulated onto respective ones of a plurality of subcarriers according to a multiple carrier modulation scheme; and introducing a group delay distortion in one or more of the plurality of subcarriers, wherein a peak-to-peak variation of the group delay distortion is greater than a guard time interval corresponding to the symbol, such that portions of the one or more of the plurality of subcarriers will be received outside of a time window corresponding to the symbol at a receiver.

In another embodiment, the invention can be characterized as a method of transmission level security in a communication system including the steps of: forming a signal to be transmitted over a communication medium; and introducing a group delay distortion in the signal, wherein the group delay distortion will cause sufficient signal energy to be dispersed in time outside of a nominal window of time corresponding to a signal feature of the signal at a corresponding receiver, wherein frequency bin splattering will occur in a Fourier transform of the receiver.

In a further embodiment, the invention can be characterized as a method of transmission level security for a communication system including the steps of: receiving a signal comprising a plurality of subcarriers representing a symbol and having been transmitted according to a multiple carrier modulation scheme, wherein a respective one or more of the plurality of subcarriers has undergone a predetermined group delay distortion, wherein a peak-to-peak variation of the delay of the predetermined group delay distortion is greater than a guard time corresponding to the symbol such that portions of the one or more of the plurality of subcarriers would fall outside of a time window associated with the symbol; and removing the predetermined group delay distortion from the one or more of the plurality of subcarriers such that all of the plurality of subcarriers fit within the time window associated with the symbol.

In an additional embodiment, the invention can be characterized as a method of transmission level security for time windowed communication systems including the steps of: receiving a signal, wherein the signal has been undergone a predetermined group delay distortion, wherein the predetermined group delay distortion is such that sufficient signal energy will be received outside of a nominal window of time corresponding to a signal feature of the signal such that will cause frequency bin splattering in a Fourier transform; and removing the group delay distortion from the signal such that the signal fits within the nominal window of time.

In an added embodiment, the invention can be characterized as a transmitter implementing transmission level security for wireless communications including a baseband modulator producing digital baseband signals representing data symbols and modulated on a plurality of subcarriers and a time dispersive all-pass filter coupled to the baseband

modulator. The time dispersive all-pass filter applies a group delay distortion upon a respective one or more of the plurality of subcarriers. A peak-to-peak variation of the group delay distortion is greater than a guard time corresponding to a time window of each of the data symbols such that a receiver will receive portions of the one or more of the plurality of subcarriers outside of the time window.

In a supplementary embodiment, the invention can be characterized as a method of transmission level security in a communication system including the steps of: forming an orthogonal frequency division multiplexed (OFDM) symbol comprising a plurality of subcarriers to be transmitted over a communication medium; introducing a group delay distortion in one or more of the plurality of subcarriers by passing the symbol through one or more time-dispersive all-pass filters, wherein a peak-to-peak variation of the group delay distortion is greater than a guard time interval corresponding to the symbol, such that portions of the one or more of the plurality of subcarriers will be moved outside of a nominal window of time corresponding to the symbol destroying orthogonality between respective ones of the plurality of subcarriers, whereby a receiver's ability to retrieve the information bits from the symbol is impaired; modulating the symbol; converting the symbol to radio frequency; transmitting the symbol; receiving the symbol; converting the symbol to baseband; demodulating the symbol; and removing the group delay distortion in the one or more of the plurality of subcarriers by passing the symbol through another one or more time-dispersive all-pass filters, wherein the other one or more time-dispersive all-pass filters is the inverse of the one or more time-dispersive all-pass filters, such that each of the plurality of subcarriers will fit within the nominal window of time corresponding to the symbol and each of the plurality of subcarriers is orthogonal to each other.

### BRIEF DESCRIPTION OF THE DRAWINGS

The above and other aspects, features and advantages of the present invention will be more apparent from the following more particular description thereof, presented in conjunction with the following drawings wherein:

FIG. 1 is a functional block diagram of an orthogonal frequency division multiplexed (OFDM) communication system incorporating a group delay distortion encryption as a transmission-level security technique according to an embodiment of the invention;

FIG. 2 is a diagram of the PHY-layer frame structure for the IEEE802.11a standard used in orthogonal frequency division multiplexed (OFDM) communications;

FIG. 3A is a graphical representation of the orthogonal frequency division multiplexed (OFDM) waveform of a transmit symbol prior to encryption in which all carriers are properly contained within the appropriate time window;

FIG. 3B is a graphical representation of the orthogonal frequency division multiplexed (OFDM) waveform of the transmit symbol of FIG. 3A after encryption by introducing a group delay distortion greater than half the guard time interval to some of the carriers such that the distorted carriers are forced outside of the appropriate time window, thereby creating significant loss of orthogonality in a conventional OFDM receiver;

FIG. 4 is a functional block diagram of the signal encryption of FIG. 1 implemented as a cascade of all-pass digital filters in accordance with another embodiment of the invention;

FIG. 5A is a graphical representation illustrating frequency bin splattering within a Fourier transform when one

orthogonal frequency division multiplexed (OFDM) subcarrier is delayed (or advanced) 10% beyond a guard time interval;

FIG. 5B is a graphical representation illustrating frequency bin splattering within a Fourier transform when one orthogonal frequency division multiplexed (OFDM) subcarrier is delayed (or advanced) 30% beyond the guard time interval;

FIG. 6 is a graphical representation of the superimposed group delay characteristics for one embodiment of the dispersion filters of FIG. 4;

FIG. 7 is a graphical representation of an optimal all-pass filter design in which in the event a receiver chooses the wrong inverse filter to correct for the group delay distortion introduced at the transmitter, significant group delay distortion will still be present;

FIG. 8 is a graphical representation of an ideal output of an autocorrelation technique performed absent noise, for example, in the preamble detection of the receiver of FIG. 1, without transmission level encryption of FIG. 1;

FIG. 9 is a graphical representation of a group delay distortion applied by the transmitter of the OFDM communication system of FIG. 1, in accordance with another embodiment of the invention;

FIG. 10 is a graphical representation of the output of the autocorrelation algorithm used in the preamble detection of FIG. 1 given a group delay distortion according to FIG. 9;

FIG. 11 is a graphical representation of the output of the autocorrelation algorithm used in the preamble detection of FIG. 1 in which a group delay distortion has been introduced that will interfere with data reception, but not preamble detection and acquisition; and

FIG. 12 is a functional block diagram of an orthogonal frequency division multiplexed (OFDM) communication system incorporating a group delay distortion encryption as a transmission-level security technique according to another embodiment of the invention.

Corresponding reference characters indicate corresponding components throughout the several views of the drawings.

### DETAILED DESCRIPTION OF THE PREFERRED EMBODIMENTS

The following description of the presently contemplated best mode of practicing the invention is not to be taken in a limiting sense, but is made merely for the purpose of describing the general principles of the invention. The scope of the invention should be determined with reference to the claims.

Referring first to FIG. 1, a functional block diagram is shown of an orthogonal frequency division multiplexed (OFDM) communication system incorporating a group delay distortion encryption as a transmission-level security technique according to an embodiment of the invention. Shown is a communication system 100 including both a transmitter 102 and a receiver 104. The transmitter 102 includes input data 106, a baseband modulator 108, an inverse fast Fourier transform 110 (hereinafter referred to as an inverse FFT 110 or simply IFFT 110), a cyclic prefix extension 112, a preamble insertion 114, a signal encryptor 116, an RF modulator 118, an upconverter 120 and a transmit antenna 122. The receiver 104 includes a receive antenna 124, a downconverter 126, an RF demodulator 128, a signal decryptor 130, a cyclic prefix removal 132, a preamble detector 134, a fast Fourier transform 136

(hereinafter referred to as FFT **136**), a baseband demodulator **138**, and output data **140** (also referred to as extracted data **140**). Further illustrated is signaling **142** traveling over a communication medium.

Within the transmitter **102**, the input data **106** is input into the baseband modulator **108**, which is coupled to the IFFT **110**. The IFFT **110** is coupled to the cyclic prefix extension **112** with is coupled to the preamble insertion **114**, which is coupled to the signal encryptor **116**. The signal encryptor **116** is coupled to the RF modulator **118**, which is coupled to the upconverter **120**, which is coupled to the transmit antenna **122**. The transmit antenna **122** is coupled to the receive antenna **124** via the communication medium. Within the receiver **104**, the receive antenna **124** is coupled to the downconverter **126**, which is coupled to the RF demodulator **128**, which is coupled to the signal decryptor **130**. The signal decryptor **130** is coupled to both the cyclic prefix removal **132** and the preamble detector **134**. The cyclic prefix removal **132** is then coupled to the FFT **136**, which is coupled to the baseband demodulator **138**, which outputs the output data **140**.

In operation, the communication system **100** employs a transmission level security encryption technique in accordance with an embodiment of the invention. In accordance with this embodiment, a signal encryptor is used to introduce a group delay distortion in the digital baseband signals prior to being modulated to RF and transmitted over the communication medium. The introduction of the group delay distortion advantageously is a PHY-layer encryption of the waveform that is being transmitted such that at least portions of the RF carriers transmitted by the transmitter arrive at the receiver outside of the expected time window required for the FFT **136** of the receiver **104**. Advantageously, according to this embodiment, the receiver **104** is equipped with such a signal decryptor **130** that removes this group delay distortion from the received digital baseband signals such that at least the portion of the RF carriers that would have been pushed outside of the expected time window of the FFT **136** (of a non-equipped receiver) will be adjusted back to fit within the expected time window. Advantageously, a receiver not equipped with such a signal decryptor **130** will be unable to adequately receive the signaling from the transmitter. This transmission level security measure is referred to as time dispersion signal encryption or TDSE.

Furthermore, in accordance with several variations of this embodiment, there are two different levels of TDSE. First, a group delay distortion having a peak-to-peak variation greater than the guard time interval associated with each data symbol is introduced such that unauthorized receivers will be able to receive the preamble, i.e., the control structures associated with the transmitted data, but will not be able to receive the data portion of the signaling or the data symbols. This PHY-level encryption technique may easily be used in combination with known bit-level encryptions, such as DES, for added security. Thus, advantageously, this PHY-level encryption technique is preferable to bit level encryptions alone because in accordance with this technique, an eavesdropper will not even be able to recover the data bits at all, and is preferably used in conjunction with a bit-level encryption. With most bit-level encryptions, the eavesdropper can at least receive the scrambled data bits. Although these received data bits are encrypted, for example, the eavesdropper may still be able to reverse engineer the encryption and recover the data. Advantageously, in this embodiment, the eavesdropper simply can not receive the data bits at all, even if transmitted without any bit level encryption.

The second level of TDSE is to introduce a larger group delay distortion such that an eavesdropper can not even detect and receive the preamble of the data frames. Typically, the peak-to-peak variation of the group delay distortion is greater than half of the length of the preamble that is used for signal detection, timing synchronization and estimation of the frequency offset. Thus, the eavesdropper can not even acquire the signaling or lock on to the frequency and timing of the signaling, i.e. the eavesdropper is powerless to recover the preamble or the transmitted data.

In preferred embodiments, this transmission level security technique is employed in wireless LAN applications, e.g., indoor wireless LAN applications. In these systems, multiple wireless devices transmit and receive sensitive data. Multiple carrier modulation schemes are advantageous over single carrier modulations in these applications. A conventional single carrier transmission scheme sends only one signal at a time using one radio frequency. On the other hand, a multiple carrier transmission scheme transmits parallel signals concurrently on multiple frequencies. This results in an efficient use of the bandwidth and provides robust communications in the presence of noise, interference and multipath. Thus, multicarrier modulations perform well in the extremely harsh multipath environment of an indoor wireless LAN application.

Recently, orthogonal frequency division multiplexing (OFDM) has been applied in the application of the wireless LAN. OFDM is a type of multiple carrier modulation that encodes data on multiple frequency carriers (also referred to as subcarriers) that are chosen to be orthogonal such that at the frequency that each of the multiple carriers is evaluated, the frequency of the other carriers is at zero. It is important that this orthogonality be preserved so that the receiver **104** can accurately extract the data from the multiple carriers. In order to do this, the transmitter and the receiver should be perfectly synchronized and the multipath needs to be adequately reduced. OFDM modulation handles the multipath channel of the indoor environment by repeating the tail of each data symbol and preceding the data symbol with the repeated portion. This introduces a guard time prior to each data symbol. The guard time is typically greater than the time it takes for the transient (i.e. the multipath) to decay. OFDM technology is well known to those skilled in the art.

OFDM for wireless LAN applications has been standardized in the IEEE802.11a standard (in the U.S.) and HiperLAN2 standard (in Europe). These are physical (PHY) layer standards that, at best, offer only data payload level encryption (i.e. bit-level encryption) while the control structures are transmitted "in the clear".

Referring briefly to FIG. 2, a diagram is shown of the PHY-layer frame structure for the IEEE802.11a standard used in orthogonal frequency division multiplexed (OFDM) communications. Shown is a frame **200** having a preamble **202** and a data portion **204**. The preamble includes a short symbol portion **206** and a long symbol portion **208**. The data portion **204** includes multiple symbols **210** (also referred to as OFDM symbols **210**), each symbol **210** having a guard time interval **212** preceding it. The frame **200** is also referred to as a PHY-layer frame or a medium access control (MAC) frame.

According to these standards, the preamble **202** is chosen which is well suited to measuring frequency errors quickly in the communication system, but is substantially less ideal for measuring precision time of signal arrival. As is well known in the art, the short symbol portion **206** is used for signal detection, diversity selection, coarse frequency offset

estimation, and timing synchronization. The long symbol portion **208** is used for channel estimation and fine frequency offset estimation. Following the preamble **202**, each OFDM symbol **210** consists of a properly time-windowed set of modulated subcarriers (e.g., sine waves) and a guard time interval **212**. This guard time interval **212** is utilized to allow the communication channel's transient to decay before transmitting the next OFDM symbol **210**. According to the IEEE 802.11a standard, this guard time interval **212** is  $0.8 \mu\text{s}$  and the symbol **210** length is  $3.2 \mu\text{s}$ . According to the HiperLAN2 standard, the guard time interval **212** is  $0.4 \mu\text{s}$  or  $0.8 \mu\text{s}$  while the symbol **210** length is  $3.2 \mu\text{s}$ . As such, the guard time interval **212** is long enough such that all reflections of the transmitted symbol **210** are adequately reduced prior to transmission of the next OFDM symbol **210**. Again, the guard time interval **212** and the frame structure of the IEEE 802.11a standard are well known in the art.

The following discussion uses the wireless LAN application using OFDM modulation under the IEEE 802.11a and HiperLAN2 PHY-layer standards having the frame **200** of FIG. 2 to describe several embodiments of the invention. The input data **106** to be transmitted to one or more receivers, e.g., receiver **104**, is input into the baseband modulator **108** which modulates the data into digital baseband signals, i.e., I and Q signals, as is known in the art. For example, the baseband modulator **108** may use, but is not limited to, binary quadrature phase shift keying (BPSK), quadrature phase shift keying (QPSK), or quadrature amplitude modulation (QAM). These digital baseband signals are input to the IFFT **110** which transforms the frequency domain digital baseband signals to time domain digital baseband signals. These signals are coupled to the cyclic prefix extension **112**, which adds a guard time interval **212** to the beginning of each OFDM data symbol **210**. This guard time interval **212** is an extension of the tail of each data symbol **210** that is made to precede each data symbol. Advantageously, this guard time interval **212** is purposely made longer than the time it takes for the transient due to reflections for a particular data symbol **210** to decay prior to the transmission of the next OFDM data symbol. In accordance with the IEEE 802.11a standard, the guard time interval **212** is  $0.8 \mu\text{s}$  while the symbol **210** length is  $3.2 \mu\text{s}$ . Next, the digital baseband signals are coupled to the preamble insertion **114**, which inserts an appropriate preamble **202** in front of a set of OFDM data symbols, each OFDM data symbol **210** having a guard time interval **212** associated therewith. Each preamble **202** and set of OFDM data symbols **210** comprise one frame **200**, e.g., one MAC frame.

Next, the digital baseband signals, i.e., the baseband OFDM signals, are passed through the signal encryptor which introduces the time dispersion signal encryption (TDSE) in accordance with several embodiments of the invention. Thus, the signal encryptor **116** introduces a group delay distortion in one or more of the individual subcarriers (e.g., sine waves) of each OFDM data symbol. According to one embodiment, the peak-to-peak group delay distortion introduced is no less than the guard time interval **212** prepended to each OFDM data symbol **210**. This will allow an eavesdropper to detect the preamble **202**, but not to receive the data bits themselves. According to another embodiment, a much larger peak-to-peak group delay distortion is introduced, which will prevent the autocorrelator of the eavesdropper's receiver from even being able to properly detect and obtain the preamble **202** of the frame **200**.

Furthermore, the signal encryptor **116** does not have to introduce this group delay distortion in all of the subcarriers

of the OFDM data symbols. For example, the signal encryptor **116** may introduce a  $+0.7 \mu\text{s}$  group delay distortion in one subcarrier (e.g., sine wave) of the OFDM data symbol, a  $+0.2 \mu\text{s}$  group delay distortion in another subcarrier of the OFDM data symbol, and a  $-0.5 \mu\text{s}$  group delay distortion in yet another of the subcarriers of the OFDM data symbol, while not introducing a group delay distortion in the remaining subcarriers. Advantageously, since each of the these subcarriers need to be received within a specific time window at the FFT **136** of the receiver **104**, some of the subcarriers will be pushed out of the FFT's effective time window (i.e., the nominal window of time of the Fourier transform). It is preferable that the peak-to-peak group delay distortion is greater than the guard time interval **212** of the symbol **210**, in this case, the peak-to-peak group delay distortion is  $1.2 \mu\text{s}$ . This will cause frequency bin splattering due to loss of orthogonality at the FFT **136**. Therefore, the FFT **136** will be unable to accurately receive the transmitted data symbols.

In preferred embodiments, the signal encryptor **116** includes one or more digital programmable all-pass filters which can be programmed to introduce a variable amount of group delay. Such all-pass filters are advantageously linear filters, such as infinite impulse response (IIR) filters, that will not add any non-linearities or amplitude distortions into the signaling. In some embodiments, the signal encryption involves a cascade of all-pass filters. Further details of the signal encryption will be described below.

Next, the OFDM signal is modulated by the IQ modulator **118** and upconverted to radio frequency (RF) by the upconverter **120** and transmitted via the transmit antenna **122** over the communication medium.

At the receiver **104**, the signaling **142** is received at the receive antenna **124**, downconverted at the downconverter **126**, and demodulated to baseband at the IQ demodulator **128**. It is at this point that a receiver equipped with a corresponding signal decryptor can compensate for the TDSE, i.e., the group delay distortions introduced at the transmitter. For the moment, assume that no signal encryption took place at the transmitter **102**, then the baseband signal would be coupled to the preamble detector **134** and the cyclic prefix removal **132**. The preamble detector **134** conventionally uses an autocorrelation algorithm which detects the presence of the signaling, estimates the frequency error of the received signaling, and also synchronizes with the timing of the preamble. According to the IEEE 802.11a standard, the short symbol portion **206** is used for this purpose. The cyclic prefix removal **132** removes the guard time interval **212** that was inserted at the cyclic prefix extension **112** of the transmitter **102**. As such, the guard time interval **212** accounts for normal time dispersion of the symbol which is introduced by the channel. This time-windows the received signaling into discrete windows of time, each containing one OFDM data symbol **210**. According to OFDM transmissions, each OFDM data symbol **210** comprises a properly time-windowed set of subcarriers.

Next, the time-windowed digital baseband signal is input to the FFT **136** which is used to convert the time domain digital baseband signal into its equivalent frequency domain digital baseband signal. As is known, the FFT **136** operates according to defined windows of time. Furthermore, the OFDM waveform is designed such that the subcarriers representing each OFDM data symbol are all contained within this window of time and orthogonality is maintained. If the timing between the transmitter and the receiver is misaligned by more than the guard time interval, one or more of the subcarriers will be pushed outside of the time

window and there will be loss of orthogonality and frequency bin splattering will occur within the FFT 136. This results in significant bit error rates, which depending on the severity of the time misalignment, will cripple the receiver's ability to recover the data 140 from the baseband demodulator 138. Thus, the timing synchronization between the transmitter 102 and the receiver 104 is critical to OFDM reception.

In order to compensate for the group delay distortions introduced at the transmitter 102, the receiver includes a signal decryptor 130. The signal decryptor 130 includes one or more all-pass filters that will remove the group delay distortion introduced into the received signaling. The all-pass filters are preferably the inverse of the one or more all-pass filters used in the signal encryption in the transmitter 102. The specific filtering used in the signal encryption and the inverse filtering used in the signal decryption is further described below with reference to FIGS. 4 through 7.

Furthermore, although this embodiment is described in the of OFDM modulation within a wireless LAN application, it is appreciated that the transmission level encryption may be applied to any communication system which uses a Fourier transform, e.g., a fast Fourier transform (FFT) and a discrete Fourier transform (DFT), at the receiver. As such, this embodiment, and other embodiments, apply to many single carrier modulation communications, and other multiple carrier modulation communication systems. As long as the receiver used evaluates the received signaling within discrete windows of time, a PHY-layer encryption technique which introduces a group delay distortion in the carrier or carriers such that at least a portion of the carrier or carriers arrive outside of the expected time window will effectively disrupt the recovery of the data.

It is also noted that several embodiments of the invention are effective in a spread spectrum system or direct sequence spread spectrum (DSSS) system, such as code division multiple access (CDMA). Such spread spectrum systems rely upon the correlation properties of the underlying spreading codes used to spread the narrowband signal into a wideband signal. The introduction of a group delay distortion into such signaling can severely degrade the correlation properties of a non-equipped receiver and also disrupt the pseudo random code tracking loops in the receiver by introducing biases and multiple false-correlation sidelobes. It is well recognized in the art that group delay distortion adversely impacts the performance of a DSSS system.

Referring briefly to FIG. 3A, a graphical representation is shown of the orthogonal frequency division multiplexed (OFDM) waveform of the transmit data symbol 210 prior to encryption in which all subcarriers are properly contained within the appropriate time window. Illustrated is an OFDM data symbol 210 properly contained within a time window 302. The OFDM data symbol 210 comprises a set of properly time-windowed subcarriers 304, 306, and 308 (also referred to as carriers or sine waves 304, 306 and 308). This is an ideal OFDM data symbol 210 prior to the introduction of group delay distortions at the signal encryptor, and also prior to the insertion of the guard time interval 212 at the cyclic prefix extension. Thus, the OFDM data symbol 210 is shown as output from the IFFT 110 of FIG. 1.

Referring briefly next to FIG. 3B, a graphical representation is shown of the orthogonal frequency division multiplexed (OFDM) waveform of the transmit symbol 210 of FIG. 3A after encryption by introducing a peak-to-peak group delay distortion greater than the guard time interval 212 to some of the subcarriers such that the distorted

subcarriers are forced outside of the appropriate time window 302, thereby creating significant loss of orthogonality in a conventional OFDM receiver. Note that subcarriers 304 and 308 have undergone a group delay distortion, while subcarrier 306 was undistorted. As such, subcarrier 304 was advanced while subcarrier 308 was retarded in time such that at least portions of the respective subcarriers 304 and 308 are "pushed" outside of the time window 302 that will be used by the FFT of the receiver. Note that although a single subcarrier may be advanced or retarded less than the guard time interval and still impair the receiver's ability to receive the data as long as the peak-to-peak group delay distortion is greater than the guard time interval. It is noted that the OFDM receiver has a limited provision for time dispersions caused by the communication medium which is handled by the guard time interval itself; however, the receiver is unable to deal with time dispersion beyond a certain point. As shown, if the dispersion is great enough (as illustrated in FIGS. 3A and 3B), some of the OFDM subcarriers, i.e. sine waves, will improperly begin after the front-edge of the time window 302 of the receiver while others will end prior to the back-edge of the time window 302 of the receiver. In either case, the signal discontinuity and absence of an integral number of subcarrier cycles will destroy the subcarrier orthogonality which will cause spectral splattering in the FFT and signal reception will be greatly harmed. Thus, the illustrated OFDM data symbol 210 of FIG. 3B is shown after the removal of the guard time interval 212 at the cyclic prefix removal 132 and prior to input to the FFT 136.

One key to making this transmission level security work is to cause the signal level dispersion such that significant signal energy falls outside of the time window 302 that the receiver must observe for each OFDM symbol 210. This is illustrated in FIG. 3B wherein subcarriers 304 and 308 fall outside of the time window 302 and will be described further below.

Referring next to FIG. 4, a functional block diagram is shown of the signal encryption of FIG. 1 implemented as a cascade of all-pass digital filters in accordance with another embodiment of the invention. Illustrated is a cascade 400 of digital all-pass filters 402 labeled as filter 1 through filter p. One way to impress (and remove) a non-constant group delay characteristic on the transmitted signal (from the received signal) is to use programmable all-pass filters 402 (also referred to as time-dispersive all-pass filters). At a minimum, the peak-to-peak group delay variation imposed should be at least as large as the guard time interval as described above. Taking this tact will largely interfere with any detection and synchronization methods that make use of the guard time interval or cyclic extension interval because of the spectral splattering or smearing introduced.

Also illustrated in FIG. 4 is the structure within each of the all-pass filters 402, which is shown as an infinite impulse response (IIR) filter. The input digital baseband signal (shown as  $V_{in}$ ) is multiplied at multiplier 404 with the tap weight  $a_k$  divided by the conjugate of the tap weight  $a_k^*$ , which is input into a delay 406 of length n. The output of delay 406 is input to summer 408. The input digital baseband signal is also multiplied at multiplier 410 with 1 divided by the conjugate of the tap weight  $a_k$  and output to the summer 408. The output of the summer 408 (shown as  $V_{out}$ ) is fed back through delay 412 and then multiplied at multiplier 414 with 1 divided by the tap weight  $a_k$  which is subtracted at summer 408. The operation of such a filter design is well understood in the art of digital filters and; thus, no further explanation is provided. Furthermore, by selecting appro-

appropriate coefficients, the delay can be varied accordingly. Additionally, it is noted that the illustration of the all-pass filter **402** is one embodiment, the skilled artist will recognize that such all-pass filter may be embodied multiple ways.

In the continuous time domain, a cascade **400** of  $M$  first-order all-pass filters **402** can be used and represented as:

$$Dly(f) = \prod_{i=1}^M \frac{1 + j2\pi(f - f_i)\tau_i}{1 - j2\pi(f - f_i)\tau_i} \quad \text{Eq. (1)}$$

where  $Dly(f)$  is the delay introduced by the cascade **400** of all-pass filters **402**,  $p$  is the number of all-pass filters **402**,  $f$  is frequency, and  $f_i$  is the center frequency of the  $i$ th all-pass filter.

In the digital domain however, the all-pass filter cascade **400** takes the form of:

$$H(z) = \frac{\sum_{i=0}^{N-1} c_i z^{N-i}}{\sum_{j=0}^{N-1} c_j z^{-i}} \quad \text{Eq. (2)}$$

where  $z = \exp(j2\pi f T_s)$ , and  $c_i$  represents the tap weights or coefficients for the  $i$ th all-pass filter. In this formulation,  $T_s$  is the time interval between digital baseband I and Q samples. In one embodiment,  $T_s$  is 40 MHz or 20 MHz, or 25 nsec and 50 nsec respectively. It is noted that the cascade **400** of all-pass filters **402** represented in Eq. (2) is an infinite impulse response (IIR) filter, the poles can significantly affect the transient response duration of the filter, but to first-order, the filter memory is at a minimum of  $NT_s$ , where  $N$  is the number of samples. At the highest sampling rate of 40 MHz,  $0.80 \mu\text{sec} * 40 \text{ MHz} = 32$  samples.

Advantageously, since the all-pass filters are linear filters, the cascade **400** of all-pass filters **402** does not introduce any non-linearities or amplitude distortions into the signaling in a transmit spectrum sense. Thus, the signal encryption appears transparent to the signaling. Additionally, such a filter design is easily digitally implemented using an ASIC or a DSP, for example.

Additionally, according to one embodiment, the signal encryption hops between the all-pass filters **402**. For example, once every MAC frame (e.g., frame **200**), a different group delay characteristic is impressed upon the transmitted data symbols (e.g., symbols **210**). This is typically done with a pseudo random number generator that is used to switch between the delay characteristics of the cascade **400**. A corresponding pseudo random number generator is used at each receiver in the network in order to switch between all-pass filters in a cascade **400** of all-pass filters that are the inverse of the all-pass filters **402**. This embodiment affords an even greater level of security since the eavesdropper must not only know the specific group delay introduced into one or more of carriers of the OFDM data symbol, but also know many specific group delay characteristics and the pattern that they change on a frame-by-frame basis.

In designing an exemplary cascade **400** of all-pass filters **402** according to a preferred embodiment, the following criteria should be observed. First, the peak-to-peak variation of the group delay distortion should be greater than the guard time interval **212** between OFDM data symbols **210**. This will interfere with normal OFDM demodulation as described above. For example, according to the IEEE 802.11a standard, the peak-to-peak variation of the group delay

distortion should be greater than  $0.8 \mu\text{sec}$ . Second, the peak-to-peak variation of the group delay distortion should be greater than the guard time interval in order to smear signal energy well into the guard time interval. Thus, there should be enough energy dispersion in time so as to fill in the guard time intervals sufficiently. Third, in order to provide a level of encryption when all-pass filters are randomly switched in between, a set of sufficiently different non-flat group delay characteristics should be created and used such that even if the receiver makes the wrong selection of correcting all-pass filters, there will still be spectral splattering in the FFT of the receiver. And, fourth, the cascade **400** of all-pass filters **402** should be digitally implemented in a digital application specific integrated circuit (ASIC).

As discussed above, in order to interfere with data reception, but not interfere with preamble detection, the peak-to-peak group variation in the group delay distortion should be greater than the guard time interval. For example, in IEEE 802.11a, the peak-to-peak variation in the group delay distortion should be greater than  $0.8 \mu\text{sec}$ . In order to interfere with preamble detection, the peak-to-peak group delay distortion should be much greater than the guard time interval, for example, greater than half of the length of the portion of the preamble that is used for preamble detection, timing synchronization and frequency offset estimation. In the IEEE 802.11a standard, this portion of the preamble is called the short symbol portion **206** and is  $8 \mu\text{sec}$  in length. Thus, the peak-to-peak group delay distortion should be greater than  $4 \mu\text{sec}$ . The first level of encryption is preferable since a new user of the network, e.g., in a wireless LAN application, may easily enter the network by acquiring the preamble in transmitted signaling. However, in the second level of encryption where the user can not receive the data or the preamble, the new user has a difficult time joining the network, since the user can not acquire the timing, unless preprogrammed with the appropriate signal decryption, i.e., the appropriate cascade of inverse all-pass filters and the algorithm to switch therebetween.

In preferred embodiments, it is not enough that the encryption system look only at the peak-to-peak variation in the group delay distortion. The cascade **400** of all-pass filters **402** should disperse sufficient energy outside of the nominal time window **302** of the receiver's FFT. As such, transmission security for OFDM is achieved by purposely spreading sufficient spectral energy outside the nominal OFDM symbol time (e.g., the nominal window of time for the symbol) such that the guard time interval can not adequately mitigate the group delay distortion. The amount of signal energy dispersion is variable, depending, for example, on the type of modulation format used. A sufficient metric of this energy dispersion or delay spread is calculated as a standard deviation of the group delay distortion based upon this energy dispersion. This is expressed mathematically as:

$$\tau_{ave} = \frac{\int_0^{\infty} S(f)\tau(f)df}{\int_0^{\infty} S(f)df} \quad \text{Eq. (3)}$$

$$\sigma_{\tau} = \sqrt{\frac{\int_0^{\infty} S(f)[\tau(f) - \tau_{ave}]^2 df}{\int_0^{\infty} S(f)df}} \quad \text{Eq. (4)}$$

where  $S(f)$  is the power spectral density of the OFDM signal,  $\tau_{ave}$  is the mean group delay,  $\tau(f)$  is the group delay at frequency  $f$ , and  $\sigma_{\tau}$  is the standard deviation of the group delay ( $\sigma_{\tau}$  is also referred to as the delay spread of the group delay distortion). If  $\sigma_{\tau}$  is less than the period of the guard

time (i.e., the guard time interval), then no substantial transmission-level security is accomplished aside from the additional group delay spread that may be introduced by the channel. If  $\sigma_\tau$  is greater than the period of the guard time, then a very effective transmission-level security is provided. However, in some embodiments, it is preferred to have  $\sigma_\tau$  greater than the guard time interval, but as small as possible.

Generally, it is desired to disperse sufficient signal energy outside of the timing window of the selected signal feature. Thus, the delay spread  $\sigma_\tau$  should be at least 10% of the time duration of the signal feature to be encrypted, preferably at least 20%, more preferably at least 30%, and most preferably at least 50%. As described above, for OFDM signal encryption of a data symbol, it is desired that the delay spread of the group delay distortion, i.e.,  $\sigma_\tau$ , be greater than the guard time interval **212** of an OFDM symbol **210**. In this case, the delay spread is at least about 25% of the time duration of the signal feature (e.g., at least the 0.8  $\mu\text{sec}$  of the 3.2  $\mu\text{sec}$  OFDM symbol in accordance with the IEEE 802.11a standard, which corresponds to the 0.8  $\mu\text{sec}$  guard time interval prepended to the OFDM symbol). In the case where the signal feature to be encrypted is the preamble or in OFDM, the portion of the preamble used for timing synchronization and frequency offset estimation, i.e., the 8.0  $\mu\text{sec}$  short symbol portion **206**, then the delay spread should also be at least 10% to at least 50% of the time duration of the particular signal feature. For example, in this case, the delay spread  $\sigma_\tau$  is at least 50% of the time duration of the signal feature (e.g., at least 4.0  $\mu\text{sec}$  of the 8.0  $\mu\text{sec}$  short symbol portion **206**). Thus, as illustrated using the specific example of the OFDM waveform, the delay spread of the group delay distortion introduced into the signaling should be such that sufficient signal energy is dispersed in time from the nominal window of time for the signal feature to be encrypted. And this occurs when the delay spread is at least 10% to at least 50% of the time duration of the signal feature to be encrypted. This results in frequency bin splattering in a Fourier transform of a non-equipped receiver.

It is noted that this applies to other multiple carrier and single carrier communications, in that a group delay distortion is introduced for a transmission level security such that the non-equipped receiver's ability to adequately intercept the signaling will be impaired. In such general cases, the signal feature of the signal to be encrypted may be a symbol, a preamble, a direct sequence spread spectrum (DSSS) chip, etc. An effective transmission level security is created when the delay spread, as defined above, of the group delay distortion is at least 10% of the time duration of the signal feature, preferably at least 20%, more preferably at least 30%, and most preferably at least 50% (at least 10% to at least 50%). As such, it is noted that the optimal amount of the delay spread of the group delay distortion is variable depending on the type of signal, e.g., OFDM, CDMA, etc., and also the signal feature of the signaling. It is noted that in the case of the signal feature being a DSSS chip, the delay spread should be at least 100% of the length of the DSSS chip.

With respect to OFDM, in terms of the individual OFDM subcarrier C/N ratio (carrier to noise ratio), the CNR to achieve a 10% symbol error rate is given in Table 1 below for different modulation formats (e.g., binary phase shift keying (BPSK), quadrature phase shift keying (QPSK), quadrature amplitude modulation (16-QAM and 64-QAM)). Table 1 assumes the IEEE 802.11a waveform with the active symbol portion of 3.2  $\mu\text{sec}$  and a guard time interval of 0.8  $\mu\text{sec}$ .

TABLE 1

Constellation	C/N, dB
BPSK	-0.8
QPSK	2.2
16-QAM	12.2
64-QAM	18.8

The 10% symbol error rate (SER) is a safe guideline at which the system begins to break due to the additional group delay encryption applied. Briefly referring next to FIG. 5A, a graphical representation is shown which illustrates frequency bin splattering within a Fourier transform. FIG. 5A illustrates when a single OFDM subcarrier is delayed (or advanced) 10% beyond the guard time interval and the spectral splattering that results. Peak **502** represents the Fourier transform output of the delayed (or advanced) OFDM subcarrier. Note that the frequency bins on either side of the frequency bin containing the peak **502** are greatly effected by the group delay distortion, i.e., significant frequency bin splattering has occurred. Ideally, as is well known in the art, the frequency bins on either side should be at much lower level than illustrated. It is noted that the representation of FIG. 5A does not account for the effect of the following (k+1) OFDM symbol which would further destroy demodulation of the present  $k^{\text{th}}$  symbol.

Next, referring briefly to FIG. 5B, a graphical representation is shown which illustrates frequency bin splattering within a Fourier transform when the OFDM subcarrier of FIG. 5A is delayed (or advanced) 30% beyond the guard time interval. Again, as seen, peak **504** represents the delayed OFDM subcarrier. In this case, there is even a further pronounced frequency bin splattering (or spectral splattering) result. Again, the bins closest to the subcarrier are impaired the most; however, the impairment reaches further across the OFDM modulation spectrum than the example of FIG. 5A. In preferred embodiments, more than one subcarrier will be advanced or delayed such that the entire OFDM modulation spectrum is effected. Additionally, it is noted that the seriousness of the group delay distortion can be further increased by using a group delay distortion characteristic that has a more rapidly varying group delay characteristic versus frequency offset (see FIG. 9 below).

Next, in principle, an almost infinite number of different group delay characteristics could be drawn for these base-band all-pass filters **402** given the delay spread as defined above in Equations (3) and (4). Table 2 below shows suggested minimum values for  $\sigma_\tau$  and the C/N ratio depending on the modulation format for OFDM communications using the IEEE 802.11a standard. It is noted that for other types of multiple carrier and single carrier modulations, the amount of group delay spread or  $\sigma_\tau$  will vary, but still should follow the rule of Equation (4) above.

TABLE 2

Constellation	C/N, dB	Minimum $\sigma_\tau$
BPSK	-0.8	2.4 $\mu\text{sec}$
QPSK	2.2	1.8 $\mu\text{sec}$
16-QAM	12.2	1.0 $\mu\text{sec}$
64-QAM	18.8	1.0 $\mu\text{sec}$

Furthermore, in order to optimize the effective encryption performance, it is preferable that the filter characteristics are sufficiently different from each other that a would-be eavesdropper would have to track the change to a new filter

characteristics for each MAC frame or loose signal synchronization or loose the signal altogether. This is further described below.

It is also noted that although in preferred embodiments, many all-pass filters **402** are cascaded, that minimally, a single all-pass filter at the transmitter and a single all-pass filter at the receiver that is the inverse of the all-pass filter at the transmitter are required to effect the signal encryption.

The following is an example of the design of the cascade **400** of all-pass filters **402**. Any number of all-pass delay filters **402**, also referred to as group delay dispersion filters, can be used in the signal encryption process and their design and use can be similarly varied to produce differing results. Regardless, all of these digital all-pass filters **402** can be mathematically represented by Eq (2).

In general, the encryption method utilizes a set of pre-computed random group delay dispersion filters **402** numbering from 1 to perhaps as high as 128 depending upon the level of encryption desired. In the general case where a large number of digital all-pass filters **402** are desired for the encryption process, the design procedure for these all-pass filters **402** consists of the following steps:

- (1) Ideally limit the  $\{c_i\}$  coefficient values to  $\pm 1$  and 0 in Eq (2) (making for a total possible number of all-pass filter combinations adequately small to permit an exhaustive search, e.g., approximately  $4.3 \times 10^7$  for  $N=16$ );
- (2) Decide upon a maximum peak-to-peak group delay variation that is allowed depending upon the level of encryption, e.g., data encryption only (e.g.,  $\pm 1 \mu\text{sec}$  for IEEE 802.11a) or data and preamble encryption (e.g.,  $\pm 5 \mu\text{sec}$  for IEEE 802.11a);
- (3) Decide upon a minimum energy dispersion standard deviation ( $\sigma_r$  in Eq. (4)) which is again dependent upon the level of encryption desired;
- (4) Exhaustively search the  $\{c_i\}$  space, retaining those choices that meet the criteria just identified;
- (5) From this reduced set of  $\{c_i\}$  solutions, compute the subset of these solutions having the maximum distance from each other as defined by:

$$\text{Distance}(i, j) = \frac{\int_0^{\infty} S(f)[\tau_i(f) - \tau_j(f)]^2 df}{\int_0^{\infty} S(f) df} \quad \text{Eq. (5)}$$

where  $S(f)$  is the power spectral density, and  $\tau_i(f)$  and  $\tau_j(f)$  are the group delay distortions at frequency  $f$  for the pair of all-pass filters  $i$  and  $j$ ;

- (6) Retain the best  $N$  all-pass filter choices that together as a pair-by-pair set achieve this objective with the distance greater than a specified minimum.

Referring next to FIG. 6, a graphical representation is shown of the superimposed group delay characteristics for one embodiment of the dispersion filters of FIG. 4. In a preferred embodiment, the cascade **400** of all-pass filters **402** for time dispersion signal encryption uses only **4** different digital filters, all of which are closely related. Each all-pass filter **402** uses a fair number of time delays, but only **2** (complex) tap weights or coefficients must be computed in each all-pass filter. The z-transform for the cascade **400** of all-pass filters **402** is represented by:

$$H(z, a, n, p) = \left[ \frac{1 + az^{-n}}{a^* + z^{-n}} \right]^p \quad \text{Eq. (6)}$$

where  $a_k$  is the tap weight or coefficient (also referred to as  $C_i$ ),  $p$  is the number of cascaded all-pass filters **402**, and  $n$  is the length of the delay in nsec (e.g., 25 or 50 nsec). Preferably, the sample rate is assumed to be 40 MHz,  $n=8$ ,  $p=8$ , and  $a_k=0.20 \cdot \exp(j 2\pi k/4)$ . The superimposed group delay characteristics for the 4 dispersion filters are shown in FIG. 6 as group delay characteristics **602**, **604**, **606** and **608**.

Referring next to FIG. 7, a graphical representation is shown of an optimal all-pass filter design in which in the event a receiver chooses the wrong inverse filter to correct for the group delay distortion introduced at the transmitter, significant group delay distortion will still be present. In order for the random frame-by-frame selection between the different dispersion filters to be effective for encryption purposes, if the receiver happens to choose the wrong inverse dispersion filter for a given frame, significant dispersion should still result. This measure can be investigated by comparing the group delay characteristics on a pair-wise basis (i.e., assume filter  $i$  for transmit but assume the inverse of filter  $j$  for receive where  $i \neq j$ ). All of the possible pairings were considered and the results for one pair of filters is illustrated in FIG. 7 as group delay characteristics **702**, **704** and **706**. Thus, as illustrated, if the receiver makes the wrong choice for the dispersion filter (inverse) to be used, serious group delay dispersion still results thereby affording good encryption properties.

Referring next to FIGS. 8–11, a level of time dispersion signal encryption which interferes with the reception of data as well as the reception of the preamble is discussed.

Referring next to FIG. 8, a graphical representation is shown of an ideal output of an autocorrelation technique performed absent noise, for example, in the preamble detector **134** of the receiver **104** of FIG. 1, without any transmission level encryption. Without the time dispersion signal encryption of several embodiments of the invention, the receiver executes an autocorrelation algorithm, e.g., in the preamble detector **134** of the receiver **104** of FIG. 1. Using IEEE 802.11a, the short symbol portion **206** of the preamble uses short symbols in which every fourth OFDM carrier is utilized. As a result, the signal is periodic with a time period of  $0.80 \mu\text{sec}$ . The length of the short symbol portion **206** is  $8 \mu\text{sec}$  however, so unless the group delay dispersion is on the order of  $4 \mu\text{sec}$  or more, the autocorrelation detection is still effective in detecting the preambles presence as well as the signals approximate frequency error. The graphical representation **800** of FIG. 8 is the autocorrelation output **802** in the absence of noise centered at  $8 \mu\text{sec}$ .

Next, FIG. 9 is a graphical representation **900** of a group delay distortion **902** vs. the frequency offset applied by the transmitter of the communication system of FIG. 1, which is greater than at least half of the length of the preamble itself. For example, it is greater than  $4.0 \mu\text{sec}$  for the IEEE 802.11a standard. This group delay distortion corresponds to a level of time dispersion signal encryption which will interfere not only with data reception, but with preamble detection and acquisition.

Next, FIG. 10 is a graphical representation **1000** of the autocorrelation output **1002** of the autocorrelation algorithm used in the preamble detection of FIG. 1 given the group delay distortion **902** of FIG. 9. As illustrated, even absent noise, the autocorrelation peak is seriously dispersed with respect to the ideal autocorrelation output **802** of FIG. 8. The autocorrelation output **1002** lacks a distinct peak and is



shifted in time from the desired location, e.g., the autocorrelation output **1002** is centered at approximately 25  $\mu\text{sec}$ , compared to 8  $\mu\text{sec}$  ideally. As such, the frequency error estimate will be severely degraded. Thus, this type of group delay distortion will not only interfere with the reception of data, but also disrupts the receiver's ability to obtain the preamble of the signaling.

Referring next to FIG. 11, a graphical representation **1100** is shown of the autocorrelation output **1102** of the autocorrelation algorithm used in the preamble detector of FIG. 1 in which only a slight group delay distortion has been introduced which will interfere with the reception of the data of the signaling but not with the reception of the preamble. For example, given a group delay distortion of  $\pm 1 \mu\text{sec}$ , which is sufficient to smear the OFDM data symbols and their respective guard times together that the unauthorized receiver will suffer loss of orthogonality (see FIGS. 3A and 3B). At the same time, as can be seen, the impact on the preamble detection and acquisition is only slightly impaired. The autocorrelation output **1102** is very close in shape to the ideal autocorrelation output **802** of FIG. 8 and is only slightly shifted in time, e.g., by about 3  $\mu\text{sec}$ .

Referring next to FIG. 12, a functional block diagram is shown of an orthogonal frequency division multiplexed (OFDM) communication system incorporating a group delay distortion encryption as a transmission-level security technique according to another embodiment of the invention. Illustrated is the OFDM communication system **1200** including a transmitter having an OFDM baseband modulator **1202**, time dispersive filters **1204** and **1206**, a mask **1208**, a pseudo random number generator **1210** (also referred to as a PN generator **1210**), an encryption administration **1212**, an RF modulator and upconverter **1214**, and a transmit antenna **122**. The system also includes a receiver having a receive antenna **124**, RF demodulator and downconverter **1216**, time dispersive inverse filters **1218** and **1220**, another mask **1222**, another pseudo random number generator **1224** (also referred to as a PN generator **1224**), and encryption administration **1226**, and the OFDM baseband demodulator **1228**.

The communication system **1200** of FIG. 12 is similar to the communication system of FIG. 1. For example, the OFDM baseband modulator **1202** includes the modulator **108**, IFFT **110**, cyclic prefix extension **112** and the preamble **114** of FIG. 1, while the time dispersive filters **1204** and **1206**, the mask **1208**, the PN generator **1210** and the encryption administration **1212** are contained within the signal encryptor **116** of FIG. 1. Likewise, in the receiver, the time dispersive inverse filters **1218** and **1220**, the mask **1222**, the PN generator **1224** and the encryption administration **1226** are part of the signal decryptor **130** of FIG. 1 and the OFDM baseband demodulator **1128** includes the cyclic prefix removal **132**, the FFT **136** and the demodulator **138** of FIG. 1.

Again, this embodiment implements the introduction of a group delay distortion in the digital baseband signals, e.g., the I and Q signals, such that one or more of the carriers of the OFDM data symbols are advanced or delayed a predetermined amount. The encryption administration **1212** controls the level of distortion to be introduced as programmed. For example, a peak-to-peak variation of the group delay distortion greater than the guard time interval will interfere with an eavesdropper's ability to recover the data, although the eavesdropper will still be able to detect and acquire the preamble of the signaling. On the other hand, a much greater peak-to-peak variation in the group delay distortion, for example, greater than half of the portion of the preamble

used for timing synchronization and frequency offset estimation (i.e., greater than half of the short symbol portion **206** or greater than 4  $\mu\text{sec}$  for the IEEE 802.11a standard), will interfere with the eavesdropper's ability to receive both the data and the preamble.

The PN generator **1210** generates a pseudo random pattern of variable group delay commands to the time dispersive filters **1204** and **1206** to hop between on a frame-by-frame basis. The mask **1208** applies the appropriate translation between the output and the input parameters needed to control the time dispersive encryption filters. There is a separate time dispersive filter **1204** and **1206** for the I and Q digital baseband signals. Each time dispersive filter **1204** and **1206** is preferably a cascade of all-pass filters, such as illustrated and discussed with reference to FIGS. 4 through 6. There is a separate cascade of filters for both the In-phase (I) digital signals and the Quadrature-phase (Q) digital signals. Both of these cascades of all-pass filters may be differently delayed with respect to each other according to the encryption administration **1212**, although preferably, both cascades of filters will be identical while varying the input parameters. The time dispersive filters **1204** and **1206** are linear all-pass filters that introduce a group delay distortion on one or more of the carriers for each OFDM data symbol. Then the baseband signals are modulated and upconverted at the RF modulator and upconverter **1214**, as is conventionally done.

At the receiver, time dispersive inverse filters **1218** and **1220** are implemented to remove the group delay distortion that was introduced at the transmitter. The time dispersive all-pass filters **1218** and **1220** are designed to be the inverse of the time dispersive filters **1204** and **1206** at the transmitter. Furthermore, the encryption administration **1226** and the PN generator **1224** operate in tandem with their counterparts at the transmitter to cause the time dispersive inverse filters to hop between different all-pass inverse filters on a frame-by-frame basis in accordance with the group delay distortion hopping at the transmitter.

As such, once the signaling has passed through the time dispersive inverse filters **1218** and **1220**, the signaling appears as normal OFDM signaling to the OFDM baseband demodulator **1228**. A receiver without a corresponding time dispersive inverse filtering to remove the group delay distortions would not be able to receive the OFDM data symbols due to loss of orthogonality and depending on the level of group delay distortion introduced, may not be able to even receive the preamble of the signaling. This creates an effective transmission security at the PHY-layer.

Furthermore, since the filtering at the transmitter and the inverse filtering at the receiver comprise linear filters, there is no additional distortion or non-linearities introduced into the system. This has an advantage of making the filtering appear transparent to the communication system **1200**. Additionally, if desired bit-level encryptions, such as DES, could be added on top of the time dispersive signal encryption used.

It is noted that in alternative embodiments, the group delay distortion as described throughout the specification may be applied at an intermediate frequency instead of in baseband, as is done by the time dispersive filters **1204**. For example, the group delay distortion may be implemented using a bandpass filter at a non-zero intermediate frequency, e.g., located in the RF modulator and upconverter **1214**. As such, a group delay distortion is introduced into the signals to be transmitted. A corresponding inverse bandpass filter is then required in the RF demodulator and downconverter **1216** to remove the group delay distortion. Thus, in these

alternative embodiments, the group delay distortion is introduced at an intermediate frequency instead of introduced in baseband by the time dispersive filters **1204**.

While the invention herein disclosed has been described by means of specific embodiments and applications thereof, numerous modifications and variations could be made thereto by those skilled in the art without departing from the scope of the invention set forth in the claims.

What is claimed is:

1. A method of transmission level security in a communication system comprising:

forming a signal to be transmitted over a communication medium; and

introducing a group delay distortion in the signal, wherein the group delay distortion will cause sufficient signal energy to be dispersed in time outside of a nominal window of time corresponding to a signal feature of the signal at a corresponding receiver, wherein frequency bin splattering will occur in a Fourier transform of the receiver.

2. The method of claim 1 wherein the sufficient signal energy to be dispersed occurs when a delay spread  $\sigma_\tau$  of the group delay distortion is greater than at least 10% of a time duration of the nominal window of time corresponding to the signal feature, wherein the delay spread is defined by:

$$\sigma_\tau = \sqrt{\frac{\int_0^8 S(f)[\tau(f) - \tau_{ave}]^2 df}{\int_0^\infty S(f) df}}$$

where S(f) is the power spectral density of the signal,  $\tau(f)$  is the group delay distortion at frequency f,  $\tau_{ave}$  is a mean group delay distortion.

3. The method of claim 2 wherein the mean group delay distortion is defined by:

$$\tau_{ave} = \frac{\int_0^\infty S(f)\tau(f) df}{\int_0^\infty S(f) df}$$

4. The method of claim 2 wherein the delay spread  $\sigma_\tau$  of the group delay distortion is greater than at least 20% of the time duration of the nominal window of time corresponding to the signal feature.

5. The method of claim 2 wherein the delay spread  $\sigma_\tau$  of the group delay distortion is greater than at least 50% of the time duration of the nominal window of time corresponding to the signal feature.

6. The method of claim 1 wherein the signal comprises a plurality of subcarriers representing a symbol, wherein the introducing comprising introducing the group delay distortion in one or more of the plurality of subcarriers, wherein a peak-to-peak variation of the group delay distortion is greater than a guard time interval associated with the symbol.

7. The method of claim 6 wherein the symbol is an orthogonal frequency division multiplexed (OFDM) symbol.

8. The method of claim 1 wherein the introducing comprises filtering the signal with a time dispersive all-pass filter.

9. The method of claim 1 further comprising:

transmitting the signal to a receiver;

receiving the signal; and

removing the group delay distortion such that the signal energy will fit within the nominal window of time corresponding to the signal.

10. The method of claim 1 wherein the signal feature comprises a symbol.

11. The method of claim 1 wherein the signal feature comprises at least a portion of a preamble of the signal.

12. A method of transmission level security for a communication system comprising:

receiving a signal comprising a plurality of subcarriers representing a symbol and having been transmitted according to a multiple carrier modulation scheme, wherein a respective one or more of the plurality of subcarriers has undergone a predetermined group delay distortion, wherein a peak-to-peak variation of the delay of the predetermined group delay distortion is greater than a guard time corresponding to the symbol such that portions of the one or more of the plurality of subcarriers would fall outside of a time window associated with the symbol; and

removing the predetermined group delay distortion from the one or more of the plurality of subcarriers such that all of the plurality of subcarriers fit within the time window associated with the symbol.

13. The method of claim 12 wherein the predetermined group delay distortion was introduced to the one or more of the plurality of subcarriers by one or more time dispersive all-pass filters, wherein the removing comprises removing the predetermined group delay distortion by applying a corresponding one or more time dispersive all-pass filters that are the inverse of respective ones of the one or more time dispersive all-pass filters.

14. The method of claim 13 wherein the plurality of subcarriers have been modulated according to orthogonal frequency division multiplexed (OFDM) modulation, wherein the removing step results in the plurality of subcarriers being orthogonal to each other.

15. The method of claim 12 wherein the removing comprises removing the predetermined group delay distortion by hopping between respective ones of a plurality of time dispersive all-pass filters for subsequent data symbols received, wherein the respective ones of the plurality of time dispersive all-pass filters are the inverse of respective ones of a plurality of time dispersive all-pass filters at a transmitter.

16. The method of claim 12 further comprising converting, prior to the removing step, the plurality of carriers to digital baseband.

17. A method of transmission level security for time windowed communication systems comprising:

receiving a signal, wherein the signal has been undergone a predetermined group delay distortion, wherein the predetermined group delay distortion is such that sufficient signal energy will be received outside of a nominal window of time corresponding to a signal feature of the signal such that will cause frequency bin splattering in a Fourier transform; and

removing the group delay distortion from the signal such that the signal fits within the nominal window of time.

18. The method of claim 17 wherein the sufficient signal energy to be dispersed occurs when a delay spread  $\sigma_\tau$  of the group delay distortion is greater than at least 10% of a time duration of the nominal window of time corresponding to the signal feature, wherein the delay spread is defined by:

$$\sigma_{\tau} = \sqrt{\frac{\int_0^{\infty} S(f) [\tau(f) - \tau_{ave}]^2 df}{\int_0^{\infty} S(f) df}}$$

where S(f) is the power spectral density of the signal, τ(f) is the group delay distortion at frequency f, τ<sub>ave</sub> is a mean group delay distortion.

19. The method of claim 18 wherein the mean group delay distortion is defined by:

$$\tau_{ave} = \frac{\int_0^{\infty} S(f) \tau(f) df}{\int_0^{\infty} S(f) df}$$

20. The method of claim wherein the delay spread σ<sub>τ</sub> of the group delay distortion is greater than at least 20% of the time duration of the nominal window of time corresponding to the signal feature.

21. The method of claim 18 wherein the delay spread σ<sub>τ</sub> of the group delay distortion is greater than at least 50% of the time duration of the nominal window of time corresponding to the signal feature.

22. The method of claim 17 wherein the signal comprises a plurality of subcarriers representing a symbol, wherein the introducing comprising introducing the group delay distortion in one or more of the plurality of subcarriers, wherein a peak-to-peak variation of the group delay distortion is greater than a guard time interval associated with the symbol.

23. The method of claim 22 wherein the symbol is an orthogonal frequency division multiplexed (OFDM) symbol.

24. The method of claim 17 wherein the removing comprises filtering the signal with a first time dispersive all-pass filter.

25. The method of claim 24 wherein the first time dispersive all-pass filter is an inverse of a second time dispersive all-pass filter, wherein the second time dispersive all-pass filter was used to introduce the predetermined group delay distortion into the signal.

26. The method of claim 17 wherein the signal feature comprises a symbol.

27. The method of claim 17 wherein the signal feature comprises at least a portion of a preamble of the signal.

28. A transmitter implementing transmission level security for wireless communications comprising:

a baseband modulator producing digital baseband signals representing data symbols and modulated on a plurality of subcarriers; and

a time dispersive all-pass filter coupled to the baseband modulator for applying a group delay distortion upon a

respective one or more of the plurality of subcarriers, wherein a peak-to-peak variation of the group delay distortion is greater than a guard time corresponding to a time window of each of the data symbols, wherein a receiver will receive portions of the one or more of the plurality of subcarriers outside of the time window.

29. The system of claim 28 the time dispersive all-pass filter comprises one of a cascade of time dispersive all-pass filters.

30. The system of claim 28 wherein the baseband modulator comprises an orthogonal frequency division multiplexed (OFDM) baseband modulator.

31. The system of claim 28 further comprising a radio frequency modulator and upconverter coupled to the time dispersive all-pass filter.

32. A method of transmission level security in a communication system comprising:

forming an orthogonal frequency division multiplexed (OFDM) symbol comprising a plurality of subcarriers to be transmitted over a communication medium;

introducing a group delay distortion in one or more of the plurality of subcarriers by passing the symbol through one or more time-dispersive all-pass filters, wherein a peak-to-peak variation of the group delay distortion is greater than a guard time interval corresponding to the symbol, such that portions of the one or more of the plurality of subcarriers will be moved outside of a nominal window of time corresponding to the symbol destroying orthogonality between respective ones of the plurality of subcarriers, whereby a receiver's ability to retrieve the information bits from the symbol is impaired;

modulating the symbol;

converting the symbol to radio frequency;

transmitting the symbol;

receiving the symbol;

converting the symbol to baseband;

demodulating the symbol; and

removing the group delay distortion in the one or more of the plurality of subcarriers by passing the symbol through another one or more time-dispersive all-pass filters, wherein the other one or more time-dispersive all-pass filters is the inverse of the one or more time-dispersive all-pass filters, such that each of the plurality of subcarriers will fit within the nominal window of time corresponding to the symbol and each of the plurality of subcarriers is orthogonal to each other.

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